Exhibit 1021

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Wireless LANs

TGn Channel Models

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Abstract

This document provides the channel models to be used for the High Throughput Task Group (TGn).

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Revision History

Date	Version	Description of changes
1/9/04	01	Paragraph added in Sec. 4.1 describing *K*-factor simulation procedure. Paragraph added in Sec. 4.5.1 describing high AP antenna placements.
3/5/04	02	Correction of autocorrelation function and coherence time formula in Sec 4.7.1 (inclusion of f_d). Equations (4) and (7) were updated.
5/4/04	03	Table IIb removed to provide consistency with updated UM (03/802r17); added table of mean and standard deviation of cluster rms delay spread in section 4.5.1; renumbered figures to be consistent.

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1. Introduction

Multiple antenna technologies are being considered as a viable solution for the next generation of mobile and wireless local area networks (WLAN). The use of multiple antennas offers extended range, improved reliability and higher throughputs than conventional single antenna communication systems. Multiple antenna systems can be generally separated into two main groups: smart antenna based systems and spatial multiplexing based multiple-input multiple-output (MIMO) systems.

Smart antenna based systems exploit multiple transmit and/or receive antennas to provide diversity gain in a fading environment, antenna gain and interference suppression. These gains translate into improvement of the spectral efficiency, range and reliability of wireless networks. These systems may have an array of multiple antennas only at one end of the communication link (e.g., at the transmit side, such as multiple-input single-output (MISO) systems; or at the receive side, such as single-input multiple-output (SIMO) systems; or at both ends (MIMO) systems). In MIMO systems, each transmit antenna can broadcast at the same time and in the same bandwidth an independent signal sub-stream. This corresponds to the second category of multi-antennas systems, referred to as spatial multiplexing-based multiple-input multiple-output (MIMO) systems. Using this technology with n transmit and n receive antennas, for example, an n-fold increase in data rate can be achieved over a single antenna system [1]. This breakthrough technology appears promising in fulfilling the growing demand for future high data rate PAN, WLAN, WAN, and 4G systems.

In this document we propose a set of channel models applicable to indoor MIMO WLAN systems. Some of the channel models are an extension of the single-input single-output (SISO) WLAN channel models proposed by Medbo et al. [2,3]. The newly developed multiple antenna models are based on the cluster model developed by Saleh and Valenzuela [4], and further elaborated upon by Spencer et al. [5], Cramer et al. [6], and Poon and Ho [7]. Indoor SISO and MIMO wireless channels were further analyzed in [8-18].

A step-wise development of the new models follows: In each of the three models (A-C) in [2] and three additional models distinct clusters were identified first. The number of clusters varies from 2 to 6, depending on the model. This finding is consistent with numerous experimentally determined results reported in the literature [4-7,9,10] and also using ray-tracing methods [8]. The power of each tap in a particular cluster was determined so that the sum of the powers of overlapping taps corresponding to different clusters corresponds to the powers of the original power delay profiles. Next, angular spread (AS), angle-of-arrival (AoA), and angle of departure (AoD) values were assigned to each tap and cluster (using statistical methods) that agree with experimentally determined values reported in the literature. Cluster AS was experimentally found to be in the 20° to 40° range [5-10], and the mean AoA was found to be random with a uniform distribution. With the knowledge of each tap power, AS, and AoA (AoD), for a given antenna configuration, the channel matrix H can be determined. The channel matrix H fully describes the propagation channel between all transmit and receive antennas. If the number of receive antennas is n and transmit antennas is m, the channel matrix H has a dimension of n x m. To arrive at channel matrix H, we use a method that employs correlation matrix and i.i.d. matrix (zero-mean unit variance independent complex Gaussian random variables). The correlation matrix for each tap is

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based on the power angular spectrum (PAS) with AS being the second moment of PAS [19,20]. To verify the newly developed model, we have calculated the channel capacity assuming the narrowband case and compared it to experimentally determined capacity results with good agreement.

The model can be used for both 2 GHz and 5 GHz frequency bands, since the experimental data and published results for both bands were used in developing the model (average, rather than frequency dependent model). However, path loss model is frequency dependent.

The paper is organized as follows. In Sec. 2 we describe SISO WLAN models. Section 3 formulates the MIMO channel matrix. Section 4 describes the clustering approach and the method for model parameters calculation. In Sec. 5 we summarize the model parameters. In Sec. 6 we briefly describe the Matlab program. Section 7 presents the antenna correlation and channel capacity results using the models, and with Sec. 8 we conclude.

2. SISO WLAN Models

A set of WLAN channel models was developed by Medbo et al. [2,3]. In [2], five delay profile models were proposed for different environments (Models A-E):

- Model A for a typical office environment, non-line-of-sight (NLOS) conditions, and 50 ns rms delay spread.
- Model B for a typical large open space and office environments, NLOS conditions, and 100 ns rms delay spread.
- Model C for a large open space (indoor and outdoor), NLOS conditions, and 150 ns rms delay spread.
- Model D, same as model C, line-of-sight (LOS) conditions, and 140 ns rms delay spread (10 dB Ricean *K*-factor at the first delay).
- Model E for a typical large open space (indoor and outdoor), NLOS conditions, and 250 ns rms delay spread.

We use models A-C together with three additional models more representative of smaller environments, such as residential homes and small offices, for our modeling purposes. The resulting models that we propose are as follows:

- Model A (optional, should not be used for system performance comparisons), flat fading model with 0 ns rms delay spread (one tap at 0 ns delay model). This model can be used for stressing system performance, occurs small percentage of time (locations).
- Model B with 15 ns rms delay spread.
- Model C with 30 ns rms delay spread.

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- Model D with 50 ns rms delay spread.
- Model E with 100 ns rms delay spread.
- Model F with 150 ns rms delay spread.

Model mapping to a particular environment is presented in table IIb.

The tables with channel coefficients (tap delays and corresponding powers) can be found in Appendix C.

The path loss model that we propose consists of the free space loss L_{FS} (slope of 2) up to a breakpoint distance and slope of 3.5 after the breakpoint distance [21]. For each of the models different break-point distance d_{BP} was chosen

$$L(d) = L_{FS}(d) \qquad d <= d_{BP}$$

$$L(d) = L_{FS}(d_{BP}) + 35 \log_{10}(d / d_{BP}) \qquad d > d_{BP} \qquad (1)$$

where d is the transmit-receive separation distance in m. The path loss model parameters are summarized in Table I. In the table, the standard deviations of log-normal (Gaussian in dB) shadow fading are also included. The values were found to be in the 3-14 dB range [16].

New Model	d_{BP} (m)	Slope before d_{BP}	Slope after d_{BP}	Shadow fading std. dev. (dB) before d_{BP} (LOS)	Shadow fading std. dev. (dB) after d_{BP} (NLOS)
A (optional)	5	2	3.5	3	4
B	5	2	3.5	3	4
C	5	2	3.5	3	5
D	10	2	3.5	3	5
E	20	2	3.5	3	6
F	30	2	3.5	3	6

Table I: Path loss model parameters

The zero-mean Gaussian probability distribution is given by

$$p(x) = \frac{1}{\sqrt{2\pi}\sigma} \exp\left(-\frac{x^2}{2\sigma^2}\right) \qquad (2)$$

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3. MIMO Matrix Formulation

We follow the MIMO modeling approach presented in [11,20] that utilizes receive and transmit correlation matrices. The MIMO channel matrix H for each tap, at one instance of time, in the A-F delay profile models can be separated into a fixed (constant, LOS) matrix and a Rayleigh (variable, NLOS) matrix [22] (4 transmit and 4 receive antennas example)

$$H = \sqrt{P}\left(\sqrt{\frac{K}{K+1}}H_F + \sqrt{\frac{1}{K+1}}H_v\right)$$
$$= \sqrt{P}\left(\sqrt{\frac{K}{K+1}}\begin{bmatrix} e^{j\phi_{11}} & e^{j\phi_{12}} & e^{j\phi_{13}} & e^{j\phi_{14}} \\ e^{j\phi_{21}} & e^{j\phi_{22}} & e^{j\phi_{23}} & e^{j\phi_{24}} \\ e^{j\phi_{31}} & e^{j\phi_{32}} & e^{j\phi_{33}} & e^{j\phi_{34}} \\ e^{j\phi_{41}} & e^{j\phi_{42}} & e^{j\phi_{43}} & e^{j\phi_{44}} \end{bmatrix} + \sqrt{\frac{1}{K+1}}\begin{bmatrix} X_{11} & X_{12} & X_{13} & X_{14} \\ X_{21} & X_{22} & X_{23} & X_{24} \\ X_{31} & X_{32} & X_{33} & X_{34} \\ X_{41} & X_{42} & X_{43} & X_{44} \end{bmatrix}\right)$$

(3)

where X_{ij} (i-th receiving and j-th transmitting antenna) are correlated zero-mean, unit variance, complex Gaussian random variables as coefficients of the variable NLOS (Rayleigh) matrix H_V, $\exp(j\phi_{ij})$ are the elements of the fixed LOS matrix H_F, K is the Ricean K-factor, and P is the power of each tap. We assume that each tap consists of a number of individual rays so that the complex Gaussian assumption is valid. P in (3) represents the sum of the fixed LOS power and the variable NLOS power (sum of powers of all taps).

To correlate the X_{ij} elements of the matrix X, the following method can be used

$$[X] = [R_{rx}]^{1/2}[H_{iid}]\left([R_{tx}]^{1/2}\right)^T$$

(4)

where R_{tx} and R_{rx} are the receive and transmit correlation matrices, respectively, and H_{iid} is a matrix of independent zero mean, unit variance, complex Gaussian random variables, and

$$[R_{tx}] = [\rho_{txij}]$$
$$[R_{rx}] = [\rho_{rxij}]$$

(5)

where ρ_{txij} are the complex correlation coefficients between i-th and j-th transmitting antennas, and ρ_{rxij} are the complex correlation coefficients between i-th and j-th receiving antennas. An alternative approach uses the *Kronecker* product of the transmit and receive correlation matrices (H_{iid} is an array in this case instead of matrix)

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$$[X] = \{[R_{tx}] \otimes [R_{rx}]\}^{1/2} [H_{iid}] \tag{6}$$

Following is an example of 4 x 4 MIMO channel transmit and receive correlation matrices

$$R_{tx} = \begin{bmatrix} 1 & \rho_{tx12} & \rho_{tx13} & \rho_{tx14} \\ \rho_{tx21} & 1 & \rho_{tx23} & \rho_{tx24} \\ \rho_{tx31} & \rho_{tx32} & 1 & \rho_{tx34} \\ \rho_{tx41} & \rho_{tx42} & \rho_{tx43} & 1 \end{bmatrix}$$

$$R_{rx} = \begin{bmatrix} 1 & \rho_{rx12} & \rho_{rx13} & \rho_{rx14} \\ \rho_{rx21} & 1 & \rho_{rx23} & \rho_{rx24} \\ \rho_{rx31} & \rho_{rx32} & 1 & \rho_{rx34} \\ \rho_{rx41} & \rho_{rx42} & \rho_{rx43} & 1 \end{bmatrix} \tag{7}$$

The complex correlation coefficient values calculation for each tap is based on the power angular spectrum (PAS) with angular spread (AS) being the second moment of PAS [19,20]. Using the PAS shape, AS, mean angle-of-arrival (AoA), and individual tap powers, correlation matrices of each tap can be determined as described in [20]. For the uniform linear array (ULA) the complex correlation coefficient at the linear antenna array is expressed as

$$\rho = R_{XX}(D) + jR_{XY}(D) \tag{8}$$

where $D = 2\pi d / \lambda$, and R_{XX} and R_{XY} are the cross-correlation functions between the real parts (equal to the cross-correlation function between the imaginary parts) and between the real part and imaginary part, respectively, with

$$R_{XX}(D) = \int_{-\pi}^{\pi} \cos(D \sin\phi) PAS(\phi) d\phi \tag{9}$$

and

$$R_{XY}(D) = \int_{-\pi}^{\pi} \sin(D \sin\phi) PAS(\phi) d\phi \tag{10}$$

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Expressions for correlation coefficients assuming uniform, truncated Gaussian, and truncated Laplacian PAS shapes can be found in [20]. To calculate the numerical values of correlation matrices we use a Matlab program developed and distributed by L. Schumacher [23] (see Sec. 6).

Next we briefly describe the various steps in our cluster modeling approach. We

- Start with delay profiles of models B-F.
- Manually identify clusters in each of the five models.
- Extend clusters so that they overlap, determine tap powers (see Appendix A).
- Assume PAS shape of each cluster and corresponding taps (Laplacian).
- Assign AS to each cluster and corresponding taps.
- Assign mean AoA (AoD) to each cluster and corresponding taps.
- Assume antenna configuration.
- Calculate correlation matrices for each tap.

In the next section we elaborate on the above steps.

4. Cluster Modeling Approach

The cluster model was introduced first by Saleh and Valenzuela [4] and later verified, extended, and elaborated upon by many other researchers in [5-10]. The received signal amplitude β_{kl} is a Rayleigh-distributed random variable with a mean-square value that obeys a double exponential decay law

$$\overline{\beta_{kl}^{\ 2}} = \overline{\beta^2(0,0)} e^{-T_l/\Gamma} e^{-\tau_{kl}/\gamma} \tag{11}$$

where $\overline{\beta^2(0,0)}$ represents the average power of the first arrival of the first cluster, T_l represents the arrival time of the lth cluster, and τ_{kl} is the arrival time of the kth arrival within the lth cluster, relative to T_l. The parameters Γ and γ determine the inter-cluster signal level rate of decay and the intra-cluster rate of decay, respectively. The rates of the cluster and ray arrivals can be determined using exponential rate laws

$$p(T_l \mid T_{l-1}) = \Lambda e^{-\Lambda(T_l - T_{l-1})} \tag{12}$$

$$p(\tau_{kl} \mid \tau_{k-1,l}) = \lambda e^{-\lambda(T_l - T_{l-1})} \tag{13}$$

where Λ is the cluster arrival rate and λ is the ray arrival rate.

For our modeling purposes we are not using the equations (11) through (13) since the delay profile characteristics are already predetermined by the model B-F delay profiles.

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4.1 Number of clusters

The number of clusters found in different indoor environments varies between 1 and 7. In [5], the average number of clusters was found to be 3 for one building, and 7 for another building. In [7] the number of clusters reported was found to be 2 for line-of-sight (LOS) and 5 for non-LOS (NLOS) conditions.

Figure 1 shows Model D delay profile with clusters outlined by exponential decay (straight line on a log-scale).

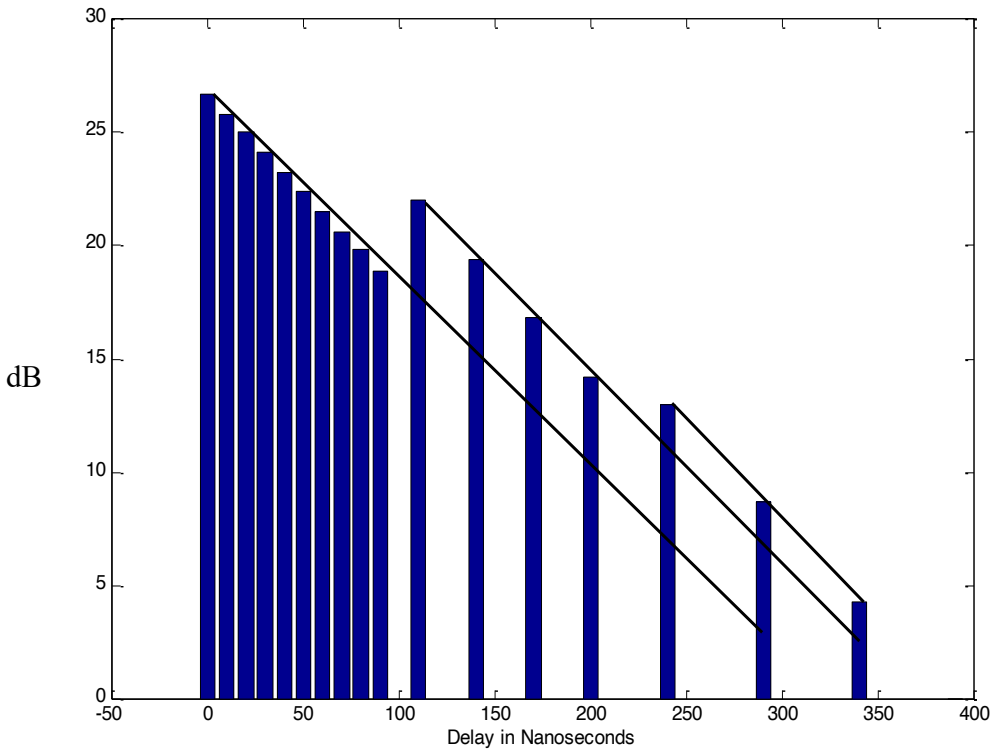

Figure 1. Model D delay profile with cluster extension (overlapping clusters).

Clearly, three clusters can be identified. For Models B, C, D, E, and F we identified (assigned) 2, 2, 3, 4 and 6 clusters, respectively. The number of clusters in each of the models B-F agrees well with the results reported in the literature. We recall that the model A consists of only one tap.

Next, we extend each cluster in B-F models so that they overlap (see Fig.1). We use a straight-line extrapolation function (in dB) on the first few visible taps of each cluster. The powers of overlapping taps were calculated so that the total sum of the powers of overlapping taps corresponding to different clusters equals to the powers of the original B-F power delay profiles. The procedure is described in detail in Appendix A.

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In Table II we summarize the channel model parameters for both line-of-sight (LOS) and non-line-of-sight (NLOS) conditions.

A (optional)	LOS/NLOS	0/ -∞	0	1 tap
B	LOS/NLOS	0 / -∞	15	2
C	LOS/NLOS	0 / -∞	30	2
D	LOS/NLOS	3 / -∞	50	3
E	LOS/NLOS	6 / -∞	100	4
F	LOS/NLOS	6 / -∞	150	6

Table II: Summary of model parameters for LOS/NLOS conditions. *K*-factor for LOS conditions applies only to the first tap, for all other taps $K = -\infty$ dB.

K-factor values for LOS conditions are based on the results presented in [39, 41] where it was found that for LOS condition, open (larger) environments have higher *K*-factors than smaller environments with close-in reflecting objects (more scattering). The LOS *K*-factor is applicable only to the first tap while all the other taps *K*-factor remain at $-\infty$ dB. LOS conditions are assumed only up to the breakpoint distance in Table I. It was also found that, for the LOS conditions, the power of the first tap relative to the other taps is larger than for the NLOS conditions [39].

The LOS component of the first tap is added on top of the NLOS component so that the total energy of the first tap for the LOS channels becomes higher than the value defined in the power delay profiles (PDP) in Appendix C. The procedure can be described as follows:

- Start with delay profiles (NLOS) as defined in tables in Appendix C.
- Add LOS component to the first tap with power according to the specified *K*-factor and 45° AoA (AoD).
- The resulting power of the first tap increases due to the added LOS component (the power of the first tap should not be scaled back to match the original NLOS PDPs).

Note that the above procedure reduces (slightly) the rms delay spread for the LOS channels when compared to the NLOS channels.

4.2 PAS Shape

The angle of arrival statistics within a cluster were found to closely match the Laplacian distribution [5,6,10]

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$$p(\theta) = \frac{1}{\sqrt{2}\sigma} e^{-\left|\sqrt{2}\theta/\sigma\right|} \tag{14}$$

where σ is the standard deviation of the PAS (which corresponds to the numerical value of AS). The Laplacian distribution is shown in Fig. 2 (a typical simulated distribution within a cluster, with AS = 30°).

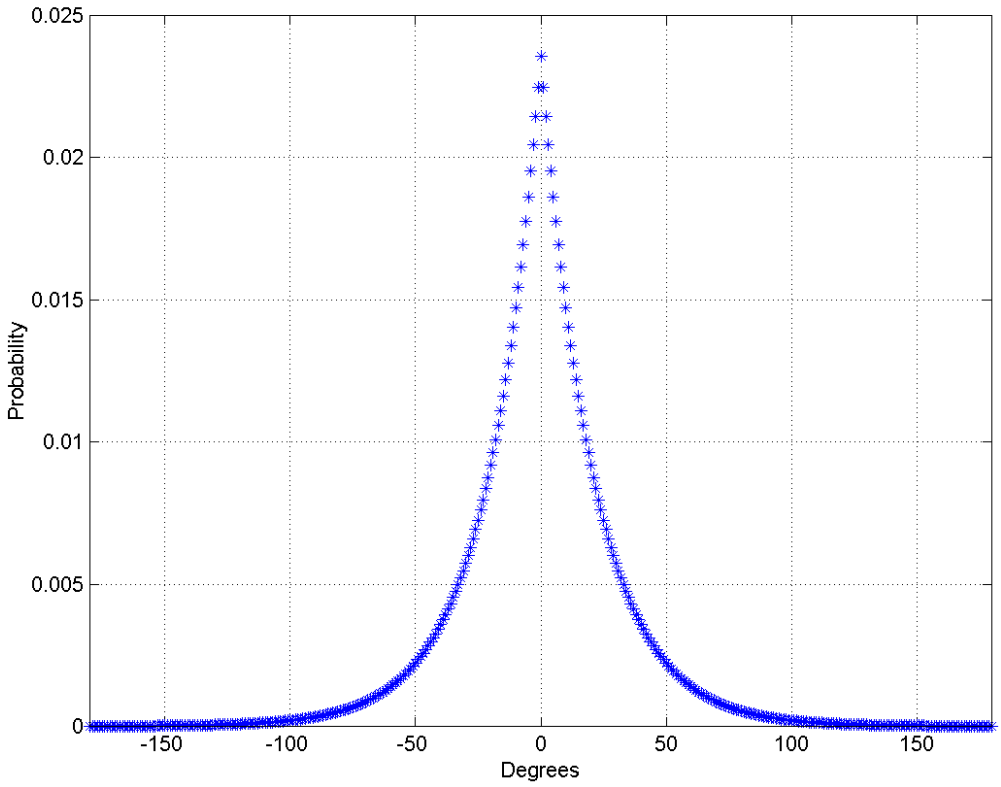

Figure 2. Example of a Laplacian distribution, AS = 30°.

4.3 Mean AoA (AoD) of Each Cluster

It was found in [5,6] that the relative cluster mean AoAs have a random uniform distribution over all angles.

In our model, we assume that the relative cluster mean AoDs also have a random uniform distribution over all angles. We assume this since for indoor WLANs, the multipath reflectors tend to be similar for both the access point (AP) and the client (STA). Note, this is usually not the case for mobile phone communications where the base station (BS) is mounted high on a tower, while the mobile station (MS) is often surrounded by local scatterers, or in the case of indoor WLAN communication when AP and STA antenna heights and surrounding environments are significantly different [30].

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For the Tables shown in Appendix C, the cluster AoAs and AoDs were determined in the following manner. Use Model D as an example, where there are 3 clusters. The 3 mean AoAs were set by randomly generating 3 values from a uniform distribution over [0,2π]. Similarly, the 3 mean cluster AoDs were set by randomly generating 3 different values from the uniform distribution over [0,2π], uncorrelated from the three AoA values.
These 6 mean values (3 AoA and 3 AoD) are then fixed and used for all future channel realizations (e.g., packet error rate performance estimation). By using fixed values, transmit and receive correlation matrices are computed only once.

The AoAs and AoDs for other models were similarly computed.

4.4 Tap Time and Angle Dependence

We assume that the channel impulse response as a function of time and angle is a separable function, h, [5,6]

$$h(t,\theta) = h(t)h(\theta) \tag{15}$$

where t is time and θ is an angle.

4.5 AS of Each Cluster

4.5.1 Azimuth AS

In [5] the mean cluster AS values were found to be 21° and 25° for two buildings measured. In [6] the mean AS value was found to be 37°. To be consistent with these findings, we select the mean cluster AS values for models A-F in the 20° to 40° range. To assign an AS value to each cluster within a particular model, we use observations from outdoor channels. For outdoor environments, it was found that the cluster rms delay spread (DS) is highly correlated (0.7 correlation coefficient) with the AS [24]. It was also found that the cluster rms delay spread and AS can be modeled as correlated log-normal random variables. We apply this intuitive finding to models B-F using the following procedure (we note that the DS are calculated from the experimental data and AS values are determined following the procedure described below)

- Calculate rms DS of each cluster, convert to dB values ($10\log_{10}n$, where n is rms delay spread in nanoseconds).
- For each model, calculate the mean rms DS and corresponding standard deviation, σ_d (dB).
- Determine the mean cluster AS in dB ($10\log_{10}m$, where m is AS in degrees) proportionally (linear dependence) to the mean cluster rms DS values using the following formula (the resulting mean AS is in the 20° to 40° range)

$$\overline{AS} = 0.32\overline{DS} + 9.88 \quad \text{(dB)} \tag{16}$$

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The model-dependent cluster DS and AS can be represented in the following form

$$DS = \overline{DS} + \sigma_d x \quad \text{(dB)} \tag{17}$$

$$AS = \overline{AS} + \sigma_a y \quad \text{(dB)} \tag{18}$$

where x and y are zero-mean, unit-variance Gaussian random variables and σ_d and σ_a are standard deviations, respectively.

- We further assume that $\sigma_a = \sigma_d$, and that the correlation coefficient between the Gaussian random variables x and y is 0.7.
- Using the following formula we can determine y, with x known

$$y = \rho x + \sqrt{1-\rho^2}\, z \tag{19}$$

where ρ is the correlation coefficient and z is an independent zero-mean unit-variance Gaussian random variable.

The above procedure results in a lower AS for models with lower rms delay spread and larger AS for models with larger rms delay spread. The resulting AS and DS at the receive side are shown in Fig. 3 for all models and clusters. For the transmit side, an independent set of AS was generated similar to the results in Fig. 3 (cluster AS at receiver does not have to necessarily match the cluster AS at the transmitter). For the model A (16)-(19) were not used since it represents a one-tap flat fading model with the following selected values: DS = 0, AoA = 45°, AoD = 45°, and AS = 40° at both transmitter and receiver.

Model	Mean Cluster DS (dB)	Std. Dev. Cluster DS (dB)
B	9.7498	1.6879
C	12.3535	0.2767
D	16.3392	0.6373
E	18.8981	0.3007
F	19.1173	1.1267

Table III: Mean and Standard Deviation of Cluster RMS Delay Spreads for each model

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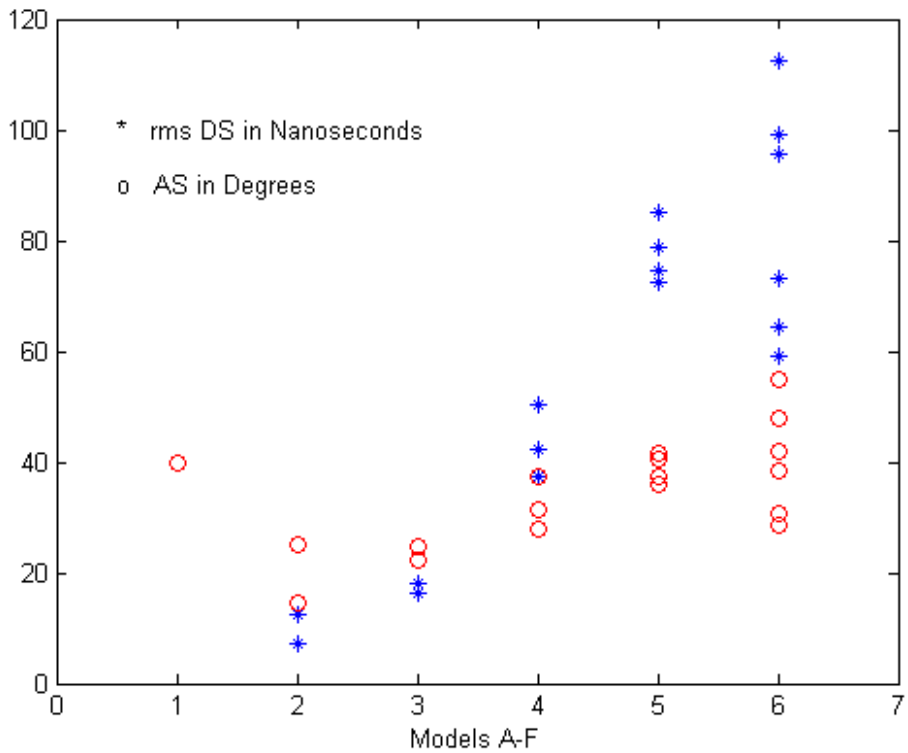

Figure 3. Cluster AS (at the receiver) and DS for all six models (A-F).

Figure 3 does not show the mean DS and mean AS (at the receiver) of (16). Rather, it shows the values determined using (17) and (18), so the shown points were stochastically determined.

Another figure could be added which shows the stochastically-determined AS at the transmitter, for each cluster's DS for all the models (A-F). Note that the mean DS for the transmitter is assumed to be equal to the mean DS for the receiver. Also, the mean AS for the transmitter is assumed to be equal to the mean AS for the receiver. In other words, the values inserted into (16) are identical for both transmit and receive. However, different random values for DS and AS are used for the transmitter versus the receiver. Equations (17) and (18) are executed once for the transmitter. Equations (17) and (18) are then executed again for the receiver.

The work in [40] addresses the cases when the AP is placed at different heights. Both 4x4 MIMO channel capacities and cluster angular widths were measured. The comparison results demonstrate the following. Firstly, the channel capacity varies with elevation by only 1-11%. This implies that the quality (or condition) of spatial channels is mostly determined by the environment and doesn't change significantly with elevation. Secondly, the cluster angular width (measured at 3 dB down from the peak) at ceiling height is only 5 degrees less than that at desktop height. Finally, the numbers of clusters seen from ceiling and desktop are 1.5 and 2.3, respectively. These numbers match those specified in the models.

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4.5.2 Elevation AS

Experimentally, it was found that the elevation AS is significantly smaller than azimuth AS. This is intuitive since most building dimensions in azimuth are considerably larger that the dimensions in elevation (building height). In our model we don't include elevation AS so that antenna array orientation applies only in a horizontal plane.

4.6 Tap AS and AoA Within Each Cluster

We assume that each tap's AS and AoA within a particular cluster has the same AS and AoA as the cluster itself. This assumption is based on the results presented in [32]. The following holds

- Each tap exhibits Laplacian PAS. Through the summation of contributing taps the corresponding cluster also exhibits a Laplacian PAS.
- The AS of the clusters determined in Sec. 4.5 should be used for each tap within a corresponding cluster.
- All the taps of a given cluster should have the same AS and AoA.

4.7 Doppler Spectrum

4.7.1 Main Temporal Doppler Component

The fading characteristics of the indoor wireless channels are very different from the one we know from the mobile case. In indoor wireless systems transmitter and receiver are stationary and people are moving in between, while in outdoor mobile systems the user terminal is often moving through an environment. As a result, a new function $S(f)$ has to be defined for indoor environments in order to fit the Doppler power spectrum measurements. $S(f)$ can be expressed as (in linear values, not dB values):

$$S(f) = \frac{1}{1 + A\left(\frac{f}{f_d}\right)^2} \tag{20}$$

where A is a constant, used to define the $0.1\,S(f)$, at a given frequency f_d, being the Doppler Spread.

$$\left(S(f)\right)\Big|_{f=f_d} = 0.1, \qquad \text{so,} \qquad A = 9 \tag{21}$$

The Doppler spread f_d is defined as

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$$f_d = \frac{v_o}{\lambda} \tag{22}$$

where v_o is the environmental speed determined from measurements that satisfy (21), and λ is the wavelength defined by

$$\lambda = \frac{c}{f_c} \tag{23}$$

where c is the light speed and f_c is the carrier frequency. The value for v_o is proposed equal to 1.2 km/h. In fact f_d values, experimentally determined in indoor environments, were found to be to be up to approximately 6 Hz at 5.25 GHz center frequency and up to approximately 3 Hz at 2.4 GHz center frequency. Represented in dB values, $S(f)$ is similar to the "Bell" shape spectrum, as shown on Fig. 4:

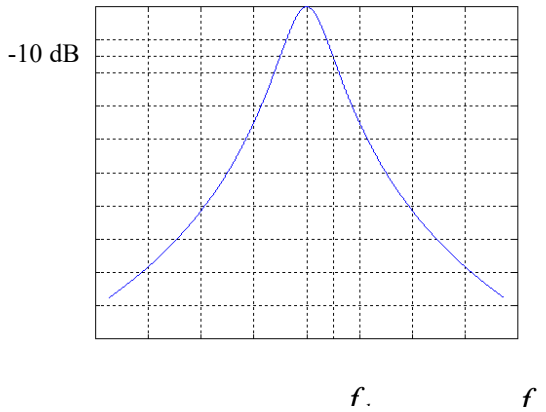

Figure 4. "Bell" shape Doppler power spectrum.

$f_{\max}$ is the maximum frequency component of the Doppler power spectrum. It limits the range of frequencies to an upper bound, and can be arbitrarily set to 5 times f_d. Figure 5 shows a typical experimental data Doppler spectrum at 5.25 GHz of a single tap (10 ns measurement system resolution) together with the fitting function of (20). Note that the measured $S(f)$ component at $f = 0$ Hz is related to the *K*-factor (DC-component) and is not included in the fitting function.

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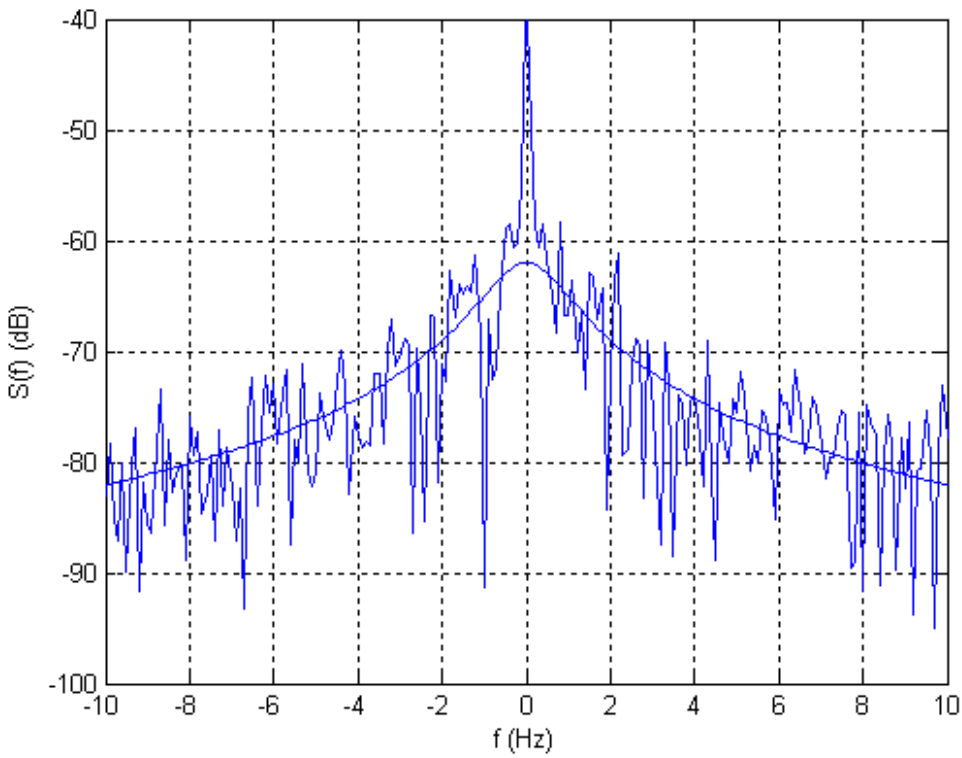

Figure 5. Measured Doppler power spectrum for a single delay tap together with the "Bell" shape fitting function.

In mobile channels, the Doppler power spectrum, $S(f)$, of the received signal can be found in [25,26], and is known as the "horn spectrum", quite different that the one in Figs. 4 and 5.

The autocorrelation function of the Bell shape spectrum is given by $R = \frac{\pi f_d}{\sqrt{A}} \cdot \exp\left(-\frac{2\pi f_d}{\sqrt{A}} \cdot \Delta t\right)$ and the coherence time is given by $T = \frac{\sqrt{A}}{2\pi f_d} \cdot \ln(2)$.

4.7.2 Doppler Component Due to a Moving Vehicle

For the channel model F, a Doppler component was included for the 3rd tap that represents a reflection from a moving vehicle. The proposed Doppler power spectrum, $S(f)$, can be expressed as (in linear values, not dB values):

$$S(f) = \frac{1}{1 + A\left(\frac{f}{f_d}\right)^2} + \frac{B}{1 + C\left(\frac{f - f_{spike}}{f_{spike}}\right)^2} \tag{24}$$

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where f_{spike} is defined as

$$f_{spike} = \frac{v_1}{\lambda} \tag{25}$$

where v_1 is the speed of a vehicle in a factory or outdoor hot-spot environment. The proposed value for v_1 is 40 km/h. The spike is present at positive frequencies only. Parameter A is set equal to 9, same as the for the "Bell" shape Doppler spectrum (21). B represents the ratio between the spike peak and the maximum of the Bell Shape. B has been determined such that the ripple on the narrowband channel responses using Model F is equal to 2-4 dB. The proposed value for B is 0.5. The reader should note that such ripple depends on the relative power between the 3rd tap and the other taps of Model F for which simple Bell shapes apply. C determines the spike bandwidth. The bandwidth is set equal to αf_{spike} where the amplitude is 10 dB below the spike peak. In this way α represents the relative bandwidth of the spike. The proposed value for α is 0.02. Since $f_{spike} >> f_d$ and $\alpha << 1$ only the second term of (24) can be adopted to determine C. Under this assumption

$$\frac{S\left(f_{spike}\left(1 \pm \frac{\alpha}{2}\right)\right)}{S\left(f_{spike}\right)} = 0.1, \text{ so,} \qquad C = \frac{36}{\alpha^2} = 90000$$

(26)

The resulting Doppler power spectrum is illustrated in Fig. 6.

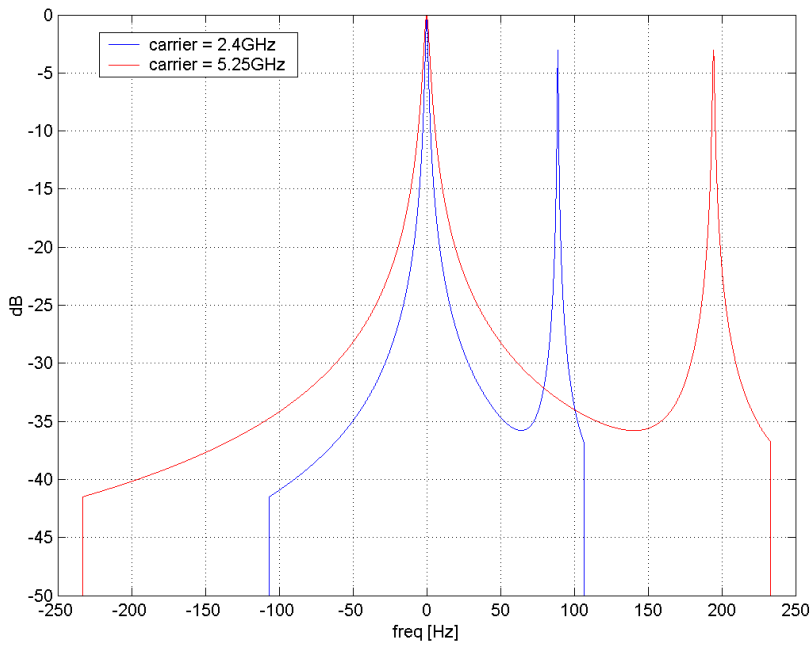

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Figure 6. Example "Bell" shape Doppler spectrum with a Doppler component due to a moving vehicle.

We note that the Doppler spectrum can be truncated similarly to the truncation in Sec. 4.7.1 (5 times f_d). Figure 7 shows narrowband channel responses using Model F. The spike due to a moving car causes a 2-4 dB signal variation.

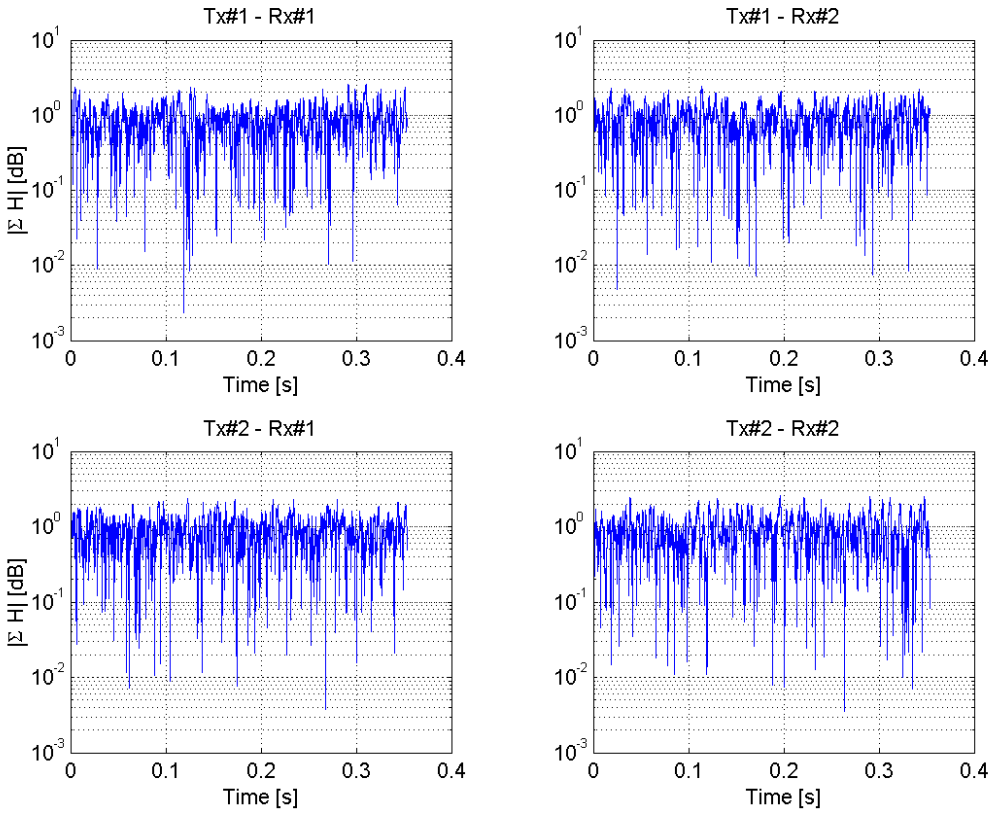

Figure 7. Narrowband impulse responses of a 2x2 MIMO channel using Model F.

4.7.3 Doppler Components Due to Fluorescent Lights

Effects of fluorescent lights on signal fading characteristics for indoor radio channels were presented in [33-37]. The presence of fluorescent lamps creates an environment where reflections are being introduced and removed at twice the power line frequency (120 Hz in the US, 100 Hz in Europe), thus creating a fast changing electromagnetic environment. The effect manifests itself in the received signal as frequency selective amplitude modulation.

This is an effect that can yield significant variation of received signal power. We include this effect in models D and E by modulating several taps in order to artificially introduce an amplitude modulation. The modulating function is randomized to yield AM distortion

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amplitudes similar to measured results, as well as various period shapes caused by random phasing of its spectral components. Furthermore, it seems adequate that the effect be introduced into models D and E (typical office, large office) as these often have omnipresent fluorescent lighting, and are affected the most from fluorescent effects.

Let

$$g(t) = \sum_{l=0}^{2} A_l \exp\{ j(4\pi(2l+1) f_m t + \varphi_l) \} \tag{27}$$

where

$g(t)$	The modulating function
A_l	Relative harmonic amplitudes
f_m	The main AC frequency
φ_l	A series of i.i.d. phase RV's $\sim U[0,2\pi)$
t	Time

We have chosen to model the fundamental tone and 2 odd harmonics (100 Hz, 300 Hz, 500 Hz in the European case), as this seems to be a good enough approximation of the modulating signal. The suggested amplitudes A_l are as follows:

Coefficient	Value [dB]
A_0	0
A_1	-15
A_2	-20

The interferer to carrier energy ratio is selected using the following random variable:

$$\frac{I}{C} = X^2 \tag{28}$$

where

$$X \sim G(0.0203, 0.0107^2) \tag{29}$$

Wherein the first figure is the mean of the Gaussian, and the second is the variance (the standard deviation squared). Figure 8 shows the CDF of the modeled I/C (interference-to-carrier ration) in green, and the measured experimental results in blue. This plot shows good agreement with the measured I/C.

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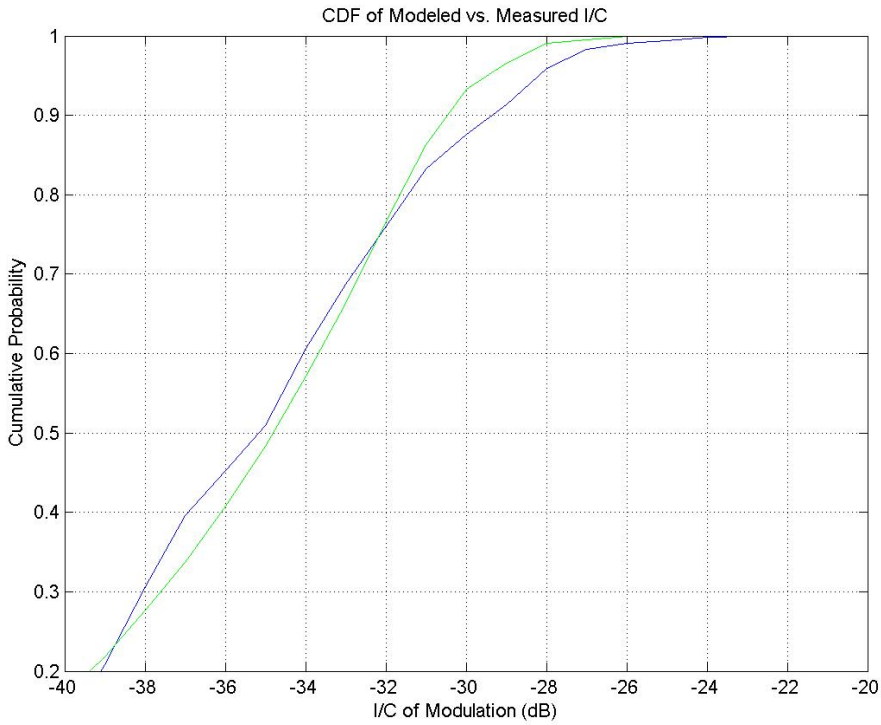

Figure 8. CDF of modeled I/C vs. measured I/C.

We modulate 3 taps in each model by the modulating function $g(t)$ in accordance with the drawn I/C. The time value of each one of these coefficients is as follows

$$c'(t) = c(t)(1 + \alpha g(t)) \tag{30}$$

where

$c(t)$	Original tap value
$c'(t)$	Modified tap value
$g(t)$	The modulating function
α	Normalization constant

The value of α is determined such that the total modulation energy (modulation in the modulated taps, compared to the entire channel response) matches the drawn random I/C. The following taps are modulated

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Model	Cluster	Tap numbers
D	2	2,4,6
E	1	3,5,7

4.8 Antennas with Different Polarizations

The cross-polarization discrimination (XPD) is defined as the ratio of the mean power received by an antenna with equal polarization orientation as the transmit antenna to the mean power received by an antenna with cross polarization orientation to the transmit antenna. In [27, 28] the XPD values were found to be in the 7-15 dB range for LOS conditions and in the 3-5 dB range for NLOS conditions. Based on these experimental results, we propose an XPD model in conjunction with (3). We assign an XPD value of 10 dB to the fixed LOS matrix H_F, and 3 dB XPD value to the variable matrix H_v. For the LOS conditions with a high K-factor, the matrix H_F dominates with 10 dB XPD. For NLOS conditions with $K = 0$, the variable matrix H_V dominates with 3 dB XPD value. Following is an example of a 2x2 MIMO system with collocated dual-polarization antennas at both transmitter and receiver [22].

$$H = \sqrt{P}\left(\sqrt{\frac{K}{K+1}}\begin{bmatrix} e^{j\phi_{11}} & \frac{1}{\sqrt{10}}e^{j\phi_{12}} \\ \frac{1}{\sqrt{10}}e^{j\phi_{21}} & e^{j\phi_{22}} \end{bmatrix} + \sqrt{\frac{1}{K+1}}\begin{bmatrix} X_{11} & \frac{1}{\sqrt{2}}X_{12} \\ \frac{1}{\sqrt{2}}X_{21} & X_{22} \end{bmatrix}\right)$$

(31)

Next, we address the correlation properties between the antennas with two different polarizations. The cross-polarization antenna correlation (between the elements of the variable part matrix in (31)) was found to be on the average significantly lower that the correlation between the antenna elements of the same polarization (co-polarized elements). The correlation for the co-polarized antenna elements separated by $\lambda/2$ was found to be in the 0.2-0.6 range, while the correlation between the cross-polarized antenna elements was found to be in the 0.0-0.2 range for typical indoor wireless channels at 5.25 GHz [31]. The dual polarization antennas yield lower antenna correlation and better condition of the fixed LOS matrix, but the XPD loss in (31) can offset the gains in some cases so that the system performance can be comparable to the single polarization MIMO system.

In this work we don't present a detailed antenna correlation model for the cross-polarized antennas.

5. Tables of Model Parameters

In Appendix C, tables show a summary of all model parameters required for the complete channel characterization, determined using methods described in Sec. 4. Each of the six

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tables representing each of the models A-F is clearly separated into distinct clusters. For each model, the following parameters are listed

- Tap Power
- Tap AoA
- Tap AoD
- Tap AS (at the receiver)
- Tap AS (at the transmitter)

For the LOS conditions the first tap contains also a fixed signal component, with the Ricean K-factor equal to values specified in Table IIa. All other taps have $K = 0$ (linear value). We specify that the fixed (LOS) signal component impinges the antenna array at the angle of 45°.

6. Matlab Program

The Matlab program that generates multiple snapshots (in time) of the channel matrix H was written by L. Schumacher [23] (together with AAU-Csys, FUND-INFO, and project IST-2000-30148 I-METRA) and is publicly available (see [23] for downloading instructions).

7. Simulated MIMO Channel Properties Using Matlab Program

In this section we determine some of the important properties of the simulated channel matrices H, specifically channel capacity. To arrive at the results, we use the narrowband assumption, which implies that the signal seen at the receiver is a summation of all taps. This assumption is valid, for example, for systems based on the orthogonal frequency division multiplexing (OFDM) modulation. For the simulation, we use the following antenna configuration system (these parameters can be used for system simulations and performance comparisons)

- 4 transmit and 4 receive antennas (4x4 MIMO system)
- Uniform linear array (ULA)
- $\lambda/2$ adjacent antenna spacing
- Isotropic antennas
- No antenna coupling effect
- All antennas with same polarization (vertical)

Channel capacity is defined as the highest transfer rate of information that can be sent with arbitrary low probability of error. We assume that the channel is known only at the receiver and that equal power is radiated from each transmitting antenna. For the n_t transmit antennas with equal transmit power and n_r receiving antennas the generalized formula for the theoretical capacity, C, can be derived [1]:

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$$C = \log_2 \det [\, I + (r/n_t)\, HH^{\dagger} \,] \quad \text{bps/Hz} \tag{32}$$

where I is an n_r x n_r identity matrix, H is an n_r x n_t matrix, $H^{\dagger}$ is its transpose conjugate, and r is the average signal-to-noise ratio (SNR).

Figure 9 shows cumulative distribution functions (CDFs) of narrowband capacity for Models A-F including i.i.d. case (channel matrix elements are i.i.d., zero-mean unit-variance complex Gaussian random variables) assuming r = 10 dB, 2000 channel realizations, and 4x4 MIMO system and NLOS conditions.

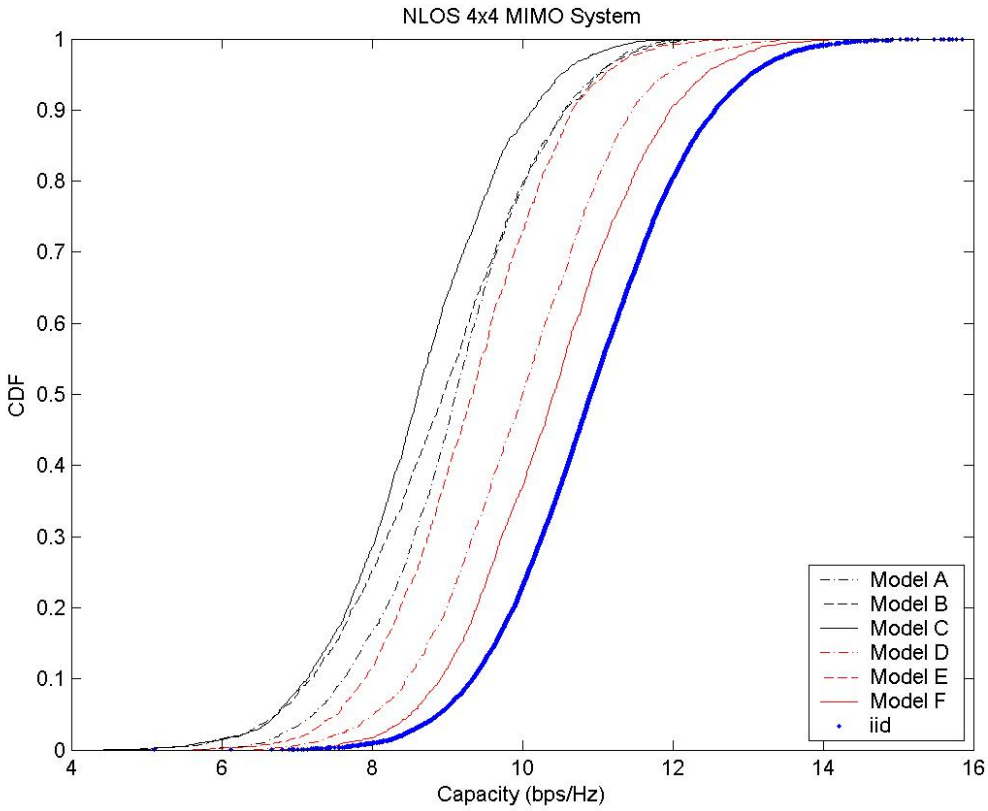

Figure 9. Simulated 4x4 MIMO narrowband capacity CDFs for the NLOS conditions.

Table III shows mean 4x4 MIMO channel capacity values for each model and corresponding % of the mean i.i.d. capacity:

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Model (NLOS)	Mean capacity in b/s/Hz	% of i.i.d. mean capacity
A (optional)	9.1	83
B	8.9	81
C	8.6	78
D	10.0	92
E	9.3	85
F	10.4	95
i.i.d.	10.9	100

Table III: 4x4 MIMO channel mean capacity for the NLOS conditions.

These results match very well with results reported in [31,33,39]. In [33] it was found experimentally that the mean capacity is approximately 80% and 95% of the 2x2 mean i.i.d. capacity for the LOS and NLOS conditions, respectively (applicable to model D). The measurement antenna spacing was λ/2. In [31, 39] it was found experimentally (λ/2 antenna spacing) that the mean capacity for the LOS case is approximately 70% of the mean 4x4 iid MIMO capacity, and for the NLOS (applicable to model E) case the mean capacity is approximately 80% of the mean 4x4 i.i.d. MIMO capacity. For the models D, E and F it is expected that the capacity is higher because of the more clusters present with wider AS when compared to the models A, B, and C. We note that MIMO systems with a smaller number of antennas are closer to the i.i.d. capacity than the systems with larger number antennas (2x2 vs. 4x4, for example). In a particular MIMO channel there may be only several significant and distinct eigenvalues available for excitation. In [39] more detailed comparison of the model to the experimental data results can be found.

For the antenna spacing of λ, the simulated mean capacity values in Table III become closer to the i.i.d. capacity (higher than 90% of the mean i.i.d. capacity).

8. Conclusion

In this document we propose a set of channel models applicable to indoor MIMO WLAN systems. The newly developed models are based on the cluster modeling approach, where tap-dependent and cluster-dependent angular and power properties are characterized. Based on these parameters, an accurate time-domain MIMO channel matrix can be obtained from the Matlab program in [23], with proper antenna correlation properties.

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Appendix A – Power roll-off parameter extraction

The objective of this Appendix is to describe a method to extend the Single-Input Single-Output (SISO) indoor Power Delay Profiles (PDP) proposed in [2] so as to encompass Multiple-Input Multiple-Output (MIMO) scenarios as well. This description will successively address the identification of clusters and the extraction of their power roll-off coefficient.

Power roll-off parameter extraction is the iterative process that finds the power roll-off coefficients for each cluster.

It starts with one of the five original models [2] that gives the channel gain A_i at each delay τ_i, i =1, …, N_{max}. For the Medbo models, N_{max} = 18. The clusters are separated such that

- Rule#1: the tap separation (in time) is constant within each cluster. It is interesting to observe that in the Medbo models the power roll-off within each cluster follows an exponential power decay law.
- Rule#2: the clusters which are the outcome of the iterative process aimed at computing the power roll-off parameters should also obey the exponential power decay law. It has been observed that, in Medbo Model B, a blind application of Rule#1 could lead to the definition of clusters whose power roll-off was actually increasing. Rule#2 is aimed at avoiding this situation. Its fulfillment requires in Medbo Model B to gather the four last taps, whose separation in time is not exactly constant, into the same cluster.
- Rule#3: the Line-of-Sight component of a Rician profile (Medbo Model D) is handled as being a cluster with a single tap.

This process has been implemented in Matlab, and we illustrate it with figures as an example. In this example the original taps are given as solid arrows with height proportional to the tap gain, the horizontal axis is excess delay, different clusters are assigned different colors to illustrate the fact that they correspond to different directional characteristics.

Next we describe the Matlab program functions:

Let's affect the working variable C with the original channel gains of the Medbo model $C \leftarrow A$.

k=1

<u>Step 1: Do a least squares fit for cluster k</u>.

We approximate the power roll-off law with an exponential power delay profile, i.e. with a function of the form $\hat{C}_{i,k} = \hat{C}_{0,k} + \gamma_k(\tau_{i,k} - \tau_{0,k})$, where $\hat{C}_{i,k}$ is the power of the i-th tap in the current cluster k, $\hat{C}_{0,k}$, γ_k are the curve fitting parameters. $\hat{C}_{i,k}$, $\hat{C}_{0,k}$ are given in dB, the time delays are given in nanoseconds (nsec) and the units of γ_k are dB/nsec.

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If this was not the last cluster proceed. Else, break.

Step 2: Extend the cluster

Following the power roll-off law found in Step 1, extend the power roll-off at taps spaced with the same separation as the one that the original cluster had. We stop introducing these extended taps when their power would be lower than the lowest allowable tap power for that profile. The original taps remain unaltered and the extensions are shown with thin shaded arrows.

Step 3: Integrate energy

Since the taps of the original model are given at specific excess delays and since we are willing to preserve this spacing in the delay domain, we need to find how much energy of the extended taps corresponds to the each of the original taps of the following clusters. These are shown as 'fat' shaded arrows because they result from the integration of one (or possibly more) thin shaded arrows. Let the fat arrows be denoted as $B_{l,k}$ for all delays τ_l beyond $\max(\tau_{i,k})$.

Step 4: Subtract energy

If the energy of the accumulated taps is lower than the energy of the original model taps, then it is subtracted (here the term 'energy' indicates that the tap powers have been appropriately integrated to account for the varying tap delay spacing). In the angular domain, this corresponds to having energy arriving both from the direction of the cluster to which the current tap belongs, and from the direction of the previous cluster(s). So $(C_{j,l}) \leftarrow C_{j,l} - B_{j,k}$.

Because we could have 3 or more clusters overlapping and energy might have to be subtracted more than once, we operate on the working variable C, instead of the initial channel gains A. This process is repeated for all clusters in the profile. Note that the subtraction is done in linear scale, not in dB.

The subtracted energy is denoted with arrows with dashed borders, while the result of the subtraction (remaining energy) is shown with patterned arrows.

k=k+1

Repeat steps 1-4 until break in step 1 (because last cluster reached).

Let us see how this procedure can be illustrated graphically using the following model as an example.

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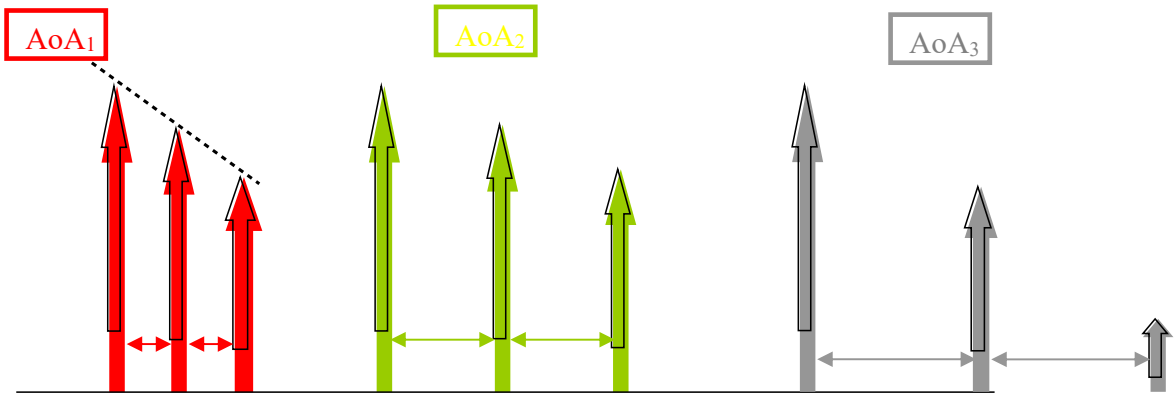

Figure A1: Original model

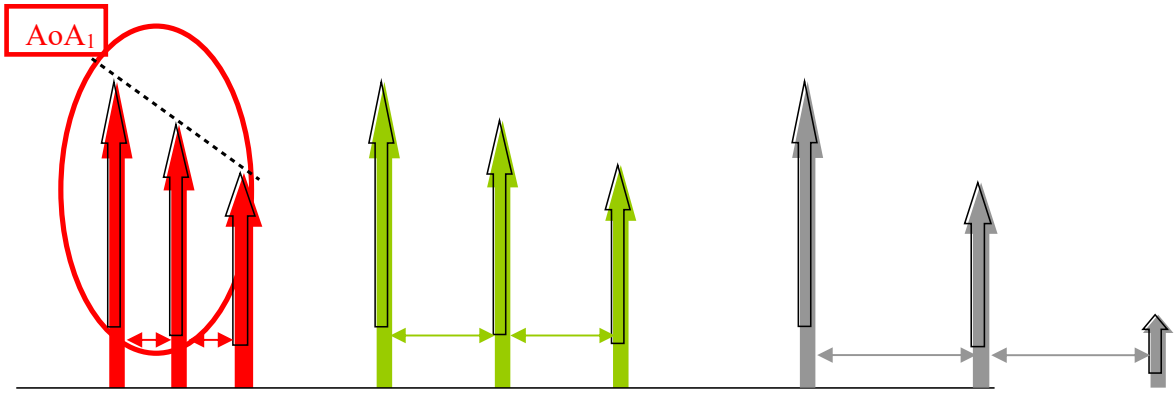

Figure A2: Step 1 (least squares fit) for cluster 1

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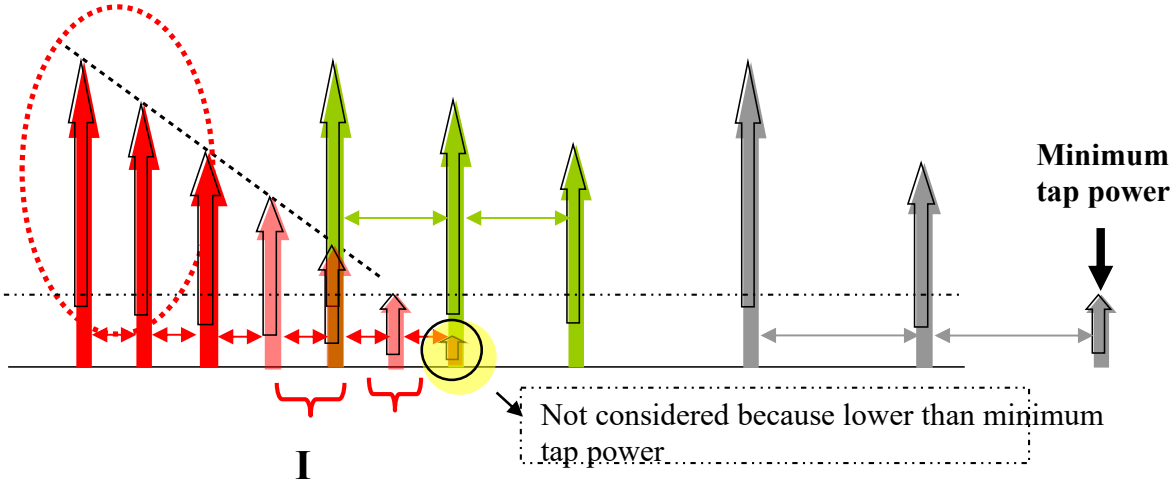

Figure A3: Step 2 (tap extension) for cluster 1

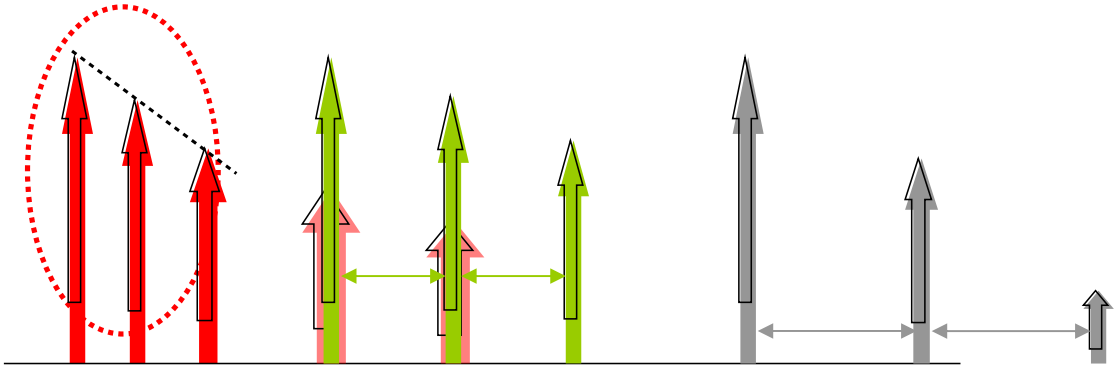

Figure A4: Step 3 (energy integration) for cluster 1

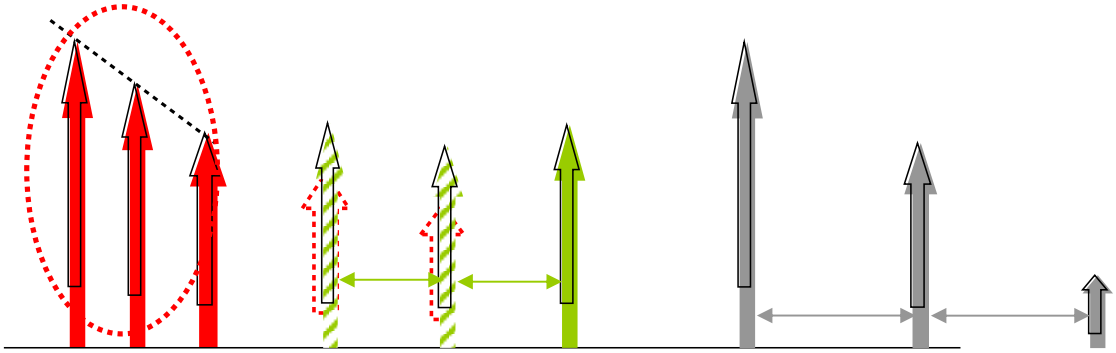

Figure A5: Step 4 (energy subtraction) for cluster 2

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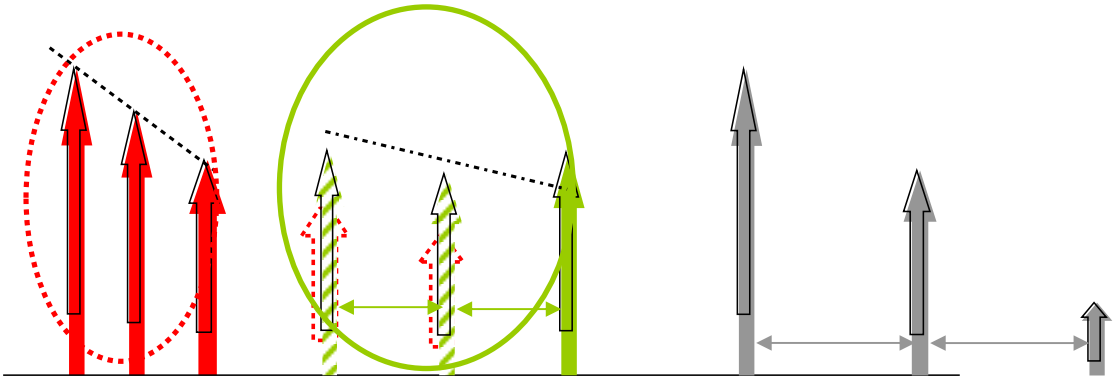

Figure A6: Step 1 (least squares fit) for cluster 2

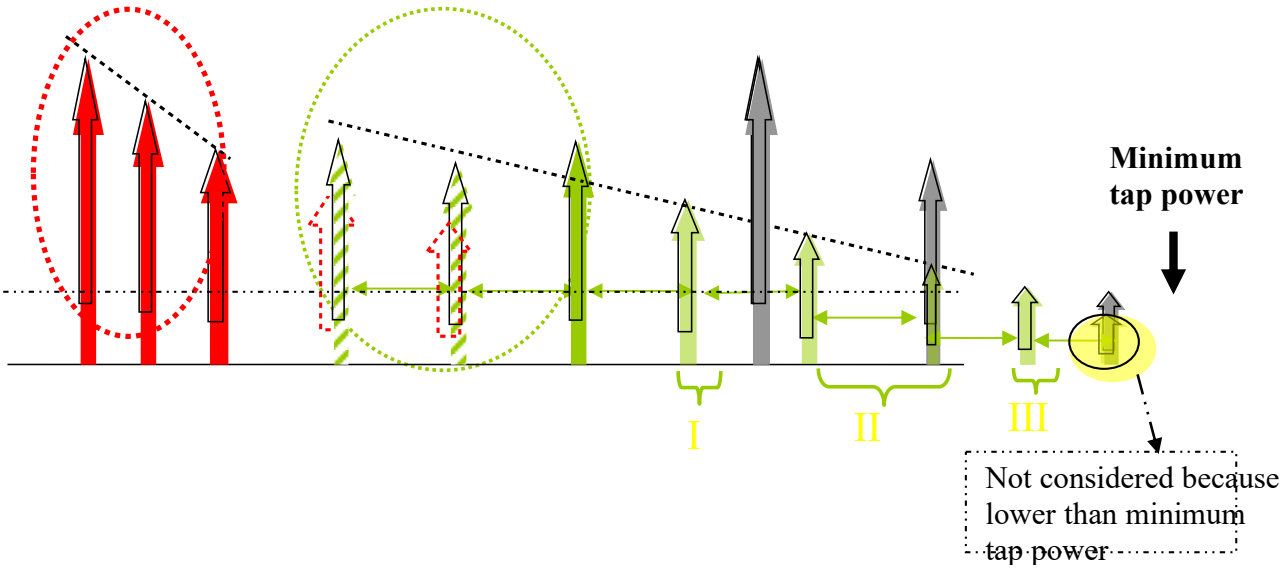

Figure A7: Step 2 (tap extension) for cluster 2

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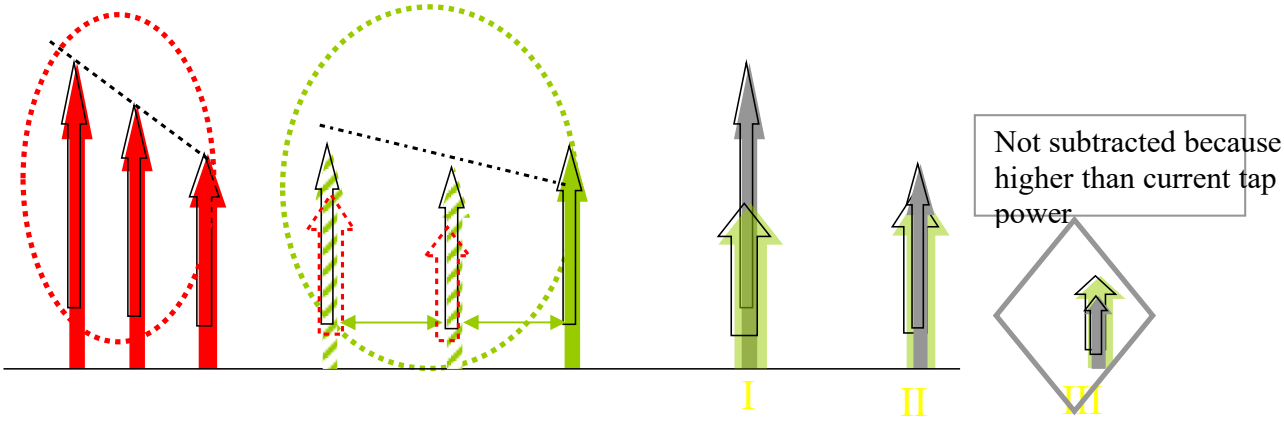

Figure A8: Step 3 (energy integration) for cluster 2

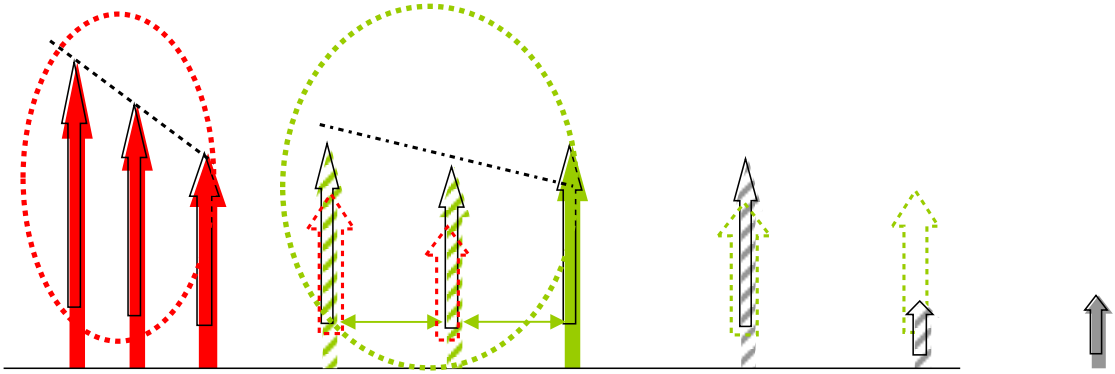

Figure A9: Step 4 (energy subtraction) for cluster 3

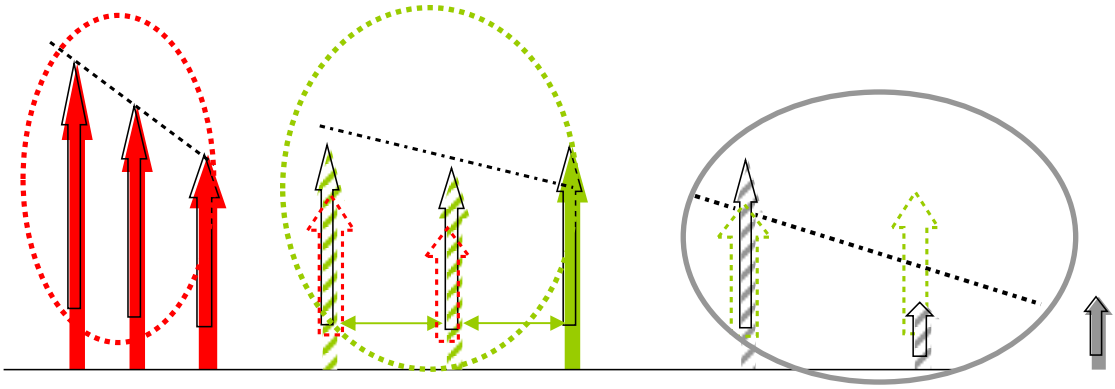

Figure A10: Step 1 (least squares fit) for cluster 3

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Appendix C – Model A (Optional Model)

	Tap index	**1**
	Excess delay [ns]	**0**
	Power [dB]	0
AoA	**AoA [°]**	45
AS (receiver)	**AS [°]**	40
AoD	**AoD [°]**	45
AS (transmitter)	**AS [°]**	40

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Appendix C – Model B

	Tap index	1	2	3	4	5	6	7	8	9
	Excess delay [ns]	0	10	20	30	40	50	60	70	80
Cluster 1	Power [dB]	0	-5.4	-10.8	-16.2	-21.7				
AoA	AoA [°]	4.3	4.3	4.3	4.3	4.3				
AS (receiver)	AS [°]	14.4	14.4	14.4	14.4	14.4				
AoD	AoD [°]	225.1	225.1	225.1	225.1	225.1				
AS (transmitter)	AS [°]	14.4	14.4	14.4	14.4	14.4				
Cluster 2	Power [dB]			-3.2	-6.3	-9.4	-12.5	-15.6	-18.7	-21.8
AoA	AoA [°]			118.4	118.4	118.4	118.4	118.4	118.4	118.4
AS	AS [°]			25.2	25.2	25.2	25.2	25.2	25.2	25.2
AoD	AoD [°]			106.5	106.5	106.5	106.5	106.5	106.5	106.5
AS	AS [°]			25.4	25.4	25.4	25.4	25.4	25.4	25.4

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Appendix C – Model C

	Tap index	1	2	3	4	5	6	7	8	9	10	11	12	13	14
	Excess delay [ns]	0	10	20	30	40	50	60	70	80	90	110	140	170	200
Cluster 1	Power [dB]	0	-2.1	-4.3	-6.5	-8.6	-10.8	-13.0	-15.2	-17.3	-19.5				
AoA	AoA [°]	290.3	290.3	290.3	290.3	290.3	290.3	290.3	290.3	290.3	290.3				
AS (receiver)	AS [°]	24.6	24.6	24.6	24.6	24.6	24.6	24.6	24.6	24.6	24.6				
AoD	AoD [°]	13.5	13.5	13.5	13.5	13.5	13.5	13.5	13.5	13.5	13.5				
AS (transmitter)	AS [°]	24.7	24.7	24.7	24.7	24.7	24.7	24.7	24.7	24.7	24.7				
Cluster 2	Power [dB]							-5.0	-7.2	-9.3	-11.5	-13.7	-15.8	-18.0	-20.2
AoA	AoA [°]							332.3	332.3	332.3	332.3	332.3	332.3	332.3	332.3
AS	AS [°]							22.4	22.4	22.4	22.4	22.4	22.4	22.4	22.4
AoD	AoD [°]							56.4	56.4	56.4	56.4	56.4	56.4	56.4	56.4
AS	AS [°]							22.5	22.5	22.5	22.5	22.5	22.5	22.5	22.5

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Appendix C – Model D

	Tap index	1	2	3	4	5	6	7	8	9	10	11	12	13	14	15	16	17	18
	Excess delay [ns]	0	10	20	30	40	50	60	70	80	90	110	140	170	200	240	290	340	390
Cluster 1	Power [dB]	0	-0.9	-1.7	-2.6	-3.5	-4.3	-5.2	-6.1	-6.9	-7.8	-9.0	-11.1	-13.7	-16.3	-19.3	-23.2		
AoA	AoA [°]	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9	158.9		
AS (receiver)	AS [°]	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7	27.7		
AoD	AoD [°]	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1	332.1		
AS (transmitter)	AS [°]	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4	27.4		
Cluster 2	Power [dB]											-6.6	-9.5	-12.1	-14.7	-17.4	-21.9	-25.5	
AoA	AoA [°]											320.2	320.2	320.2	320.2	320.2	320.2	320.2	
AS	AS [°]											31.4	31.4	31.4	31.4	31.4	31.4	31.4	
AoD	AoD [°]											49.3	49.3	49.3	49.3	49.3	49.3	49.3	
AS	AS [°]											32.1	32.1	32.1	32.1	32.1	32.1	32.1	
Cluster 3	Power [dB]															-18.8	-23.2	-25.2	-26.7
AoA	AoA [°]															276.1	276.1	276.1	276.1
AS	AS [°]															37.4	37.4	37.4	37.4
AoD	AoD [°]															275.9	275.9	275.9	275.9
AS	AS [°]															36.8	36.8	36.8	36.8

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Appendix C - Model E (1/2)

	Tap index	1	2	3	4	5	6	7	8	9	10	11	12	13	14	15	16	17	18
	Excess delay [ns]	0	10	20	30	50	80	110	140	180	230	280	330	380	430	490	560	640	730
Cluster 1	Power [dB]	-2.6	-3.0	-3.5	-3.9	-4.5	-5.6	-6.9	-8.2	-9.8	-11.7	-13.9	-16.1	-18.3	-20.5	-22.9			
AoA	AoA [°]	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7	163.7			
AS (receive)	AS [°]	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8	35.8			
AoD	AoD [°]	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6	105.6			
AS (transmit)	AS [°]	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1	36.1			
Cluster 2	Power [dB]					-1.8	-3.2	-4.5	-5.8	-7.1	-9.9	-10.3	-14.3	-14.7	-18.7	-19.9	-22.4		
AoA	AoA [°]					251.8	251.8	251.8	251.8	251.8	251.8	251.8	251.8	251.8	251.8	251.8	251.8		
AS	AS [°]					41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6		
AoD	AoD [°]					293.1	293.1	293.1	293.1	293.1	293.1	293.1	293.1	293.1	293.1	293.1	293.1		
AS	AS [°]					42.5	42.5	42.5	42.5	42.5	42.5	42.5	42.5	42.5	42.5	42.5	42.5		

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Appendix C - Model E (2/2)

Cluster 3	Power [dB]	-7.9	-9.6	-14.2	-13.8	-18.6	-18.1	-22.8		
AoA	AoA [°]	80.0	80.0	80.0	80.0	80.0	80.0	80.0		
AS	AS [°]	37.4	37.4	37.4	37.4	37.4	37.4	37.4		
AoD	AoD [°]	61.9	61.9	61.9	61.9	61.9	61.9	61.9		
AS	AS [°]	38.0	38.0	38.0	38.0	38.0	38.0	38.0		
Cluster 4	Power [dB]							-20.6	-20.5	-20.7	-24.6
AoA	AoA [°]							182.0	182.0	182.0	182.0
AS	AS [°]							40.3	40.3	40.3	40.3
AoD	AoD [°]							275.7	275.7	275.7	275.7
AS	AS [°]							38.7	38.7	38.7	38.7

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Appendix C – Model F (1/2)

	Tap index	1	2	3	4	5	6	7	8	9	10	11	12	13	14	15	16	17	18
	Excess delay [ns]	0	10	20	30	50	80	110	140	180	230	280	330	400	490	600	730	880	1050
Cluster 1	Power [dB]	-3.3	-3.6	-3.9	-4.2	-4.6	-5.3	-6.2	-7.1	-8.2	-9.5	-11.0	-12.5	-14.3	-16.7	-19.9			
AoA	AoA [°]	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1	315.1			
AS (receive)	AS [°]	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0	48.0			
AoD	AoD [°]	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2	56.2			
AS (transmit)	AS [°]	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6	41.6			
Cluster 2	Power [dB]					-1.8	-2.8	-3.5	-4.4	-5.3	-7.4	-7.0	-10.3	-10.4	-13.8	-15.7	-19.9		
AoA	AoA [°]					180.4	180.4	180.4	180.4	180.4	180.4	180.4	180.4	180.4	180.4	180.4	180.4		
AS	AS [°]					55.0	55.0	55.0	55.0	55.0	55.0	55.0	55.0	55.0	55.0	55.0	55.0		
AoD	AoD [°]					183.7	183.7	183.7	183.7	183.7	183.7	183.7	183.7	183.7	183.7	183.7	183.7		
AS	AS [°]					55.2	55.2	55.2	55.2	55.2	55.2	55.2	55.2	55.2	55.2	55.2	55.2		
Cluster 3	Power [dB]									-5.7	-6.7	-10.4	-9.6	-14.1	-12.7	-18.5			
AoA	AoA [°]									74.7	74.7	74.7	74.7	74.7	74.7	74.7			
AS	AS [°]									42.0	42.0	42.0	42.0	42.0	42.0	42.0			
AoD	AoD [°]									153.0	153.0	153.0	153.0	153.0	153.0	153.0			
AS	AS [°]									47.4	47.4	47.4	47.4	47.4	47.4	47.4			

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Appendix C – Model F (2/2)

Cluster 4	Power [dB]	-8.8	-13.3	-18.7							
AoA	AoA [°]	251.5	251.5	251.5							
AS	AS [°]	28.6	28.6	28.6							
AoD	AoD [°]	112.5	112.5	112.5							
AS	AS [°]	27.2	27.2	27.2							
Cluster 5	Power [dB]			-12.9	-14.2						
AoA	AoA [°]			68.5	68.5						
AS	AS [°]			30.7	30.7						
AoD	AoD [°]			291.0	291.0						
AS	AS [°]			33.0	33.0						
Cluster 6	Power [dB]					-16.3	-21.2				
AoA	AoA [°]					246.2	246.2				
AS	AS [°]					38.2	38.2				
AoD	AoD [°]					62.3	62.3				
AS	AS [°]					38.0	38.0				

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